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# Grid-Connected Control Strategy of Five-Level Inverter Based on Passive E-L Model

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**Abstract:** At present, the research on five-level inverters mainly involves the modulation algorithm and topology, and few articles study the five-level inverter from the control strategy. In this paper, the nonlinear passivity-based control (PBC) method is proposed for single-phase uninterruptible power supply inverters. The proposed PBC method is based on an energy shaping and damping injection idea, which is performed to regulate the energy flow of an inverter to a desired level and to assure global asymptotic stability, respectively. Furthermore, this paper presents a control algorithm based on the theory of passivity that gives an inverter in a photovoltaic system additional functions: power factor correction, harmonic currents compensation, and the ability to stabilize the system under varying injection damping. Finally, the effectiveness of the PBC method in terms of both stability and harmonic distortion is verified by the simulation and experiments under resistive and inductive loads.

**Keywords:** five-level inverter; passive E-L model; energy function; damping injection; SPWM

## 1. Introduction

Recently, an effort to extend the scope of the applications of multilevel inverters to clean energy harnessing from photovoltaic arrays and fuel cells has also been pursued, wherein their superior harmonic performance and ability to support independent maximum power point tracking are advantages noted for these lower voltage implementations [1–4]. For high-voltage energy conversion, multilevel inverters are viewed as the preferred topological solutions compared to the traditional two-level inverter bridge because of their many associated advantages, including reduced semiconductor voltage stress, improved harmonic performance, and reduced electromagnetic interference [5,6]. The conventional multilevel converters are mainly divided into three types: neutral-point-clamped (NPC) inverter, flying capacitor (FC) inverter, and cascaded H-bridge (CHB) inverter. Many papers focus on the NPC inverter, which has found widespread use in active filters, renewable energy conversion systems, and traction motor applications [7–15].

In the literature, numerous modulation techniques have been proposed to obtain the inverter output voltage nearing a perfect sinusoidal waveform. Several modulation techniques have been proposed for reducing harmonics and minimizing switching losses for NPC inverters. The modulation methods for NPC inverters can be classified according to switching frequencies: (a) Space Vector Modulation (SVM); (b) Phase Shifted PWM; and (c) Level Shifted PWM. Among these, SVM helps in the good utilization of DC link voltage and lower current ripples. However, with a higher number of voltage levels, the complexity of choosing a switching state increases as the redundancy of the switching state increases. A level shifted modulation scheme consists of triangular carriers which are vertically shifted. The total harmonic distortion (THD) of phase-shifted modulation is much higher

than that of the level shifted technique. Therefore, level shifted modulation is considered in this paper [16–19].

With the advance of classical control theory and modern control theory, Proportional Integral (PI) control, Proportional Resonant (PR) control and sliding mode control are applied to the control of the inverter. To some extent, these methods can solve some problems. However, as the complexity and coupling of the system increase, these methods have been unable to meet the demand [20–22]. The authors of [23] proposed a deadbeat control strategy. Although the method provides a very fast dynamic response, it is not robust to the parameter variations, which may adversely affect the performance. In the literature [24], adaptive controls are applicable to the control of the inverter. This method has important advantages such as eliminating the sensitive error, ensuring that the transfer function of the controller is not changed, and improving the control performance of the system. However, the predicted value of the grid-impedance is difficult to ascertain. The authors of [25] proposed a sliding mode control strategy. The control algorithm can improve the robustness of the system and hold a superior practical value. However, variable switching frequency, steady-state error in the output voltage, and chattering are the main drawbacks of this method. Furthermore, the constant sliding gain results in a static sliding line, which leads to insufficient dynamic responses during load transients.

The aforementioned control methods offer various advantages and disadvantages related to dynamic response, robustness against parameter variations, steady-state error, and stability. The common disadvantage is that they do not take into consideration the energy dissipation properties of the inverter, which are inherently imposed by its physical structure. In order to implement the nonlinear control of power electronic devices, passivity-based control (PBC) theory has been applied to the control of the inverter and has achieved a good control effect [26,27]. In the literature [28], it is noted that PBC strategy can improve the dynamic and static characteristics of the system, which also has strong robustness to parameter changes. In the literature [29], the passivity-based control has better robustness and dynamics compared with traditional PI control. In the literature [30], PBC strategy has a fast dynamic response compared with the droop control, which can improve the stability of the system. The literature [31] proposes that passivity-based control (PBC) can simplify the control algorithm, which has a high anti-perturbation reaction to the parameter change in contrast with the traditional vector control.

At present, the research on the five-level inverter mainly involves the modulation algorithm and topology, and few articles study it with the control strategy. In this paper, passivity-based control is introduced to the system of the five-level inverter for the first time. Firstly, the mathematical model of the five-level inverter is deduced by the topological structure and the switching function. Then, the function expression of the passive E-L model can be derived by selecting the appropriate energy function and the damping injection, which combines with the Sinusoidal Pulse Width Modulation (SPWM) algorithm to drive the switch of the inverter. Finally, PBC strategy was compared with the traditional PI control through simulation software, and the results have been analyzed. Meanwhile, the validity of the control strategy based on passive Euler (E-L) model is also verified by the prototype experiment.

## 2. Topology and Mathematical Mode

### 2.1. Topology

Figure 1 showed the grid-connected system of the single-stage, three-phase, diode-clamped, five-level inverter. The equivalent resistances of the system are  $R_a$ ,  $R_b$ , and  $R_c$ , and the equivalent inductors are  $L_a$ ,  $L_b$ , and  $L_c$ . Further,  $R_a = R_b = R_c = R$ , and  $L_a = L_b = L_c = L_f$ .  $C_1 = C_2 = C_3 = C_4 = C$  is the polar film capacitor between the DC stack buses. The voltage of the DC side is  $U_{dc}$ .  $I_{dc}$  denotes the current from the DC-link to the inverter.  $T_{A1}$ – $T_{A8}$ ,  $T_{B1}$ – $T_{B8}$ , and  $T_{C1}$ – $T_{C8}$  are the eight switches on the arms of phases A, B, and C respectively.  $V_{A1}$ – $V_{A6}$ ,  $V_{B1}$ – $V_{B6}$ , and  $V_{C1}$ – $V_{C6}$  are the six clamp diodes on

the arms of phases A, B, and C respectively.  $S_A$ ,  $S_B$ , and  $S_C$  are the switch signals of each arm on the phases A, B, and C respectively. Among them, the switch signals of the arm on phase A are  $S_{A1}$ ,  $S_{A2}$ ,  $S_{A3}$ ,  $S_{A4}$ ,  $S_{A5}$ ,  $S_{A6}$ ,  $S_{A7}$ , and  $S_{A8}$ . Likewise, the switch signals of phase B and phase C can be obtained.  $U_{eA}$ ,  $U_{eB}$ , and  $U_{eC}$  denote the grid side AC voltages.

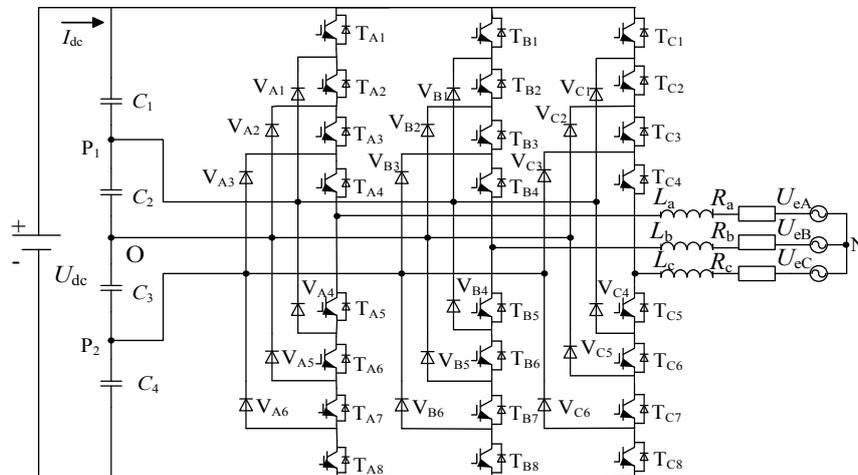


Figure 1. The topology of the diode-clamped five-level inverter.

### 2.2. Working Principle

The five-level inverter has a variety of working methods according to the switch sequence. Taking phase A as an example to explain its working principle:

- (1)  $T_{A1}$ ,  $T_{A2}$ ,  $T_{A3}$ , and  $T_{A4}$  shut down at the same time;  $T_{A5}$ ,  $T_{A6}$ ,  $T_{A7}$ , and  $T_{A8}$  switch on at the same time; and then the output phase voltage of the inverter is  $+U_{dc}/2$  and  $S_A = +2$ .
- (2)  $T_{A2}$ ,  $T_{A3}$ ,  $T_{A4}$ , and  $T_{A5}$  shut down at the same time;  $T_{A1}$ ,  $T_{A6}$ ,  $T_{A7}$ , and  $T_{A8}$  switch on at the same time; and then the output phase voltage of the inverter is  $+U_{dc}/4$  and  $S_A = +1$ .
- (3)  $T_{A3}$ ,  $T_{A4}$ ,  $T_{A5}$ , and  $T_{A6}$  shut down at the same time, and  $T_{A1}$ ,  $T_{A2}$ ,  $T_{A7}$ , and  $T_{A8}$  switch on at the same time. O point and N point have the same potential at the same moment, so the output phase voltage of the inverter is 0. Meanwhile,  $S_A = 0$ .
- (4)  $T_{A4}$ ,  $T_{A5}$ ,  $T_{A6}$ , and  $T_{A7}$  shutdown at the same time;  $T_{A1}$ ,  $T_{A2}$ ,  $T_{A3}$ , and  $T_{A8}$  switch on at the same time; and the output phase voltage of the inverter is  $-U_{dc}/4$  and  $S_A = -1$ .
- (5)  $T_{A5}$ ,  $T_{A6}$ ,  $T_{A7}$ , and  $T_{A8}$  shut down at the same time;  $T_{A1}$ ,  $T_{A2}$ ,  $T_{A3}$ , and  $T_{A4}$  switch on at the same time; and the output phase voltage of the inverter is  $-U_{dc}/2$  and  $S_A = -2$ .

### 2.3. Mathematical Model

Assuming that the opening state of the switch is 0 and the closing state is 1, the penta-state switching function  $S_k$  can be decomposed into eight two-state switching functions, as in Equation (1).

$$S_k = \begin{cases} +2 \Leftrightarrow S_{k1} = 1, S_{k2} = 1, S_{k3} = 1, S_{k4} = 1, S_{k5} = 0, S_{k6} = 0, S_{k7} = 0, S_{k8} = 0 \\ +1 \Leftrightarrow S_{k1} = 0, S_{k2} = 1, S_{k3} = 1, S_{k4} = 1, S_{k5} = 1, S_{k6} = 0, S_{k7} = 0, S_{k8} = 0 \\ 0 \Leftrightarrow S_{k1} = 0, S_{k2} = 0, S_{k3} = 1, S_{k4} = 1, S_{k5} = 1, S_{k6} = 1, S_{k7} = 0, S_{k8} = 0 \\ -1 \Leftrightarrow S_{k1} = 0, S_{k2} = 0, S_{k3} = 0, S_{k4} = 1, S_{k5} = 1, S_{k6} = 1, S_{k7} = 1, S_{k8} = 0 \\ -2 \Leftrightarrow S_{k1} = 0, S_{k2} = 0, S_{k3} = 0, S_{k4} = 0, S_{k5} = 1, S_{k6} = 1, S_{k7} = 1, S_{k8} = 1 \end{cases} \quad (1)$$

where the subscript  $k = A, B, C$ .

The mathematical model of the five-level inverter in the static  $a$ - $b$ - $c$  frame can be derived as:

$$\begin{cases} L_f \frac{di_k}{dt} + Ri_k - [(S_{k1} + S_{k2})U_{C1} - (S_{k7} + S_{k8})U_{C4}] + U_{ON} = -U_{ek} \\ C \frac{dU_{C1}}{dt} + S_{A1}i_A + S_{A2}i_A + S_{B1}i_B + S_{B2}i_B + S_{C1}i_C + S_{C2}i_C = I_{dc} \\ C \frac{dU_{C4}}{dt} - S_{A1}i_A - S_{A2}i_A - S_{B1}i_B - S_{B2}i_B - S_{C1}i_C - S_{C2}i_C = I_{dc} \end{cases} \quad (2)$$

Among them,

$$U_{ON} = \frac{1}{5} [(S_{A1} + S_{A2} + S_{B1} + S_{B2} + S_{C1} + S_{C2})U_{C1} - (S_{A7} + S_{A8} + S_{B7} + S_{B8} + S_{C7} + S_{C8})U_{C4}] \quad (3)$$

where  $U_{C1}$  and  $U_{C4}$  are the voltages of the capacitors  $C_1$  and  $C_4$  in the DC side, respectively, and  $i_A$ ,  $i_B$ , and  $i_C$  are the three-phase current of the inverter.

After the coordinate transformation, the mathematical model of the five-level inverter in the dq rotation coordinate is [32–34]:

$$\begin{cases} L_f \frac{di_d}{dt} - \omega L_f i_q + Ri_d - [(S_{d1} + S_{d2})U_{C1} - (S_{d7} + S_{d8})U_{C4}] = -U_{ed} \\ L_f \frac{di_q}{dt} + \omega L_f i_d + Ri_q - [(S_{q1} + S_{q2})U_{C1} - (S_{q7} + S_{q8})U_{C4}] = -U_{eq} \\ \frac{3}{5} C \frac{dU_{C1}}{dt} + (S_{d1} + S_{d2})i_d + (S_{q1} + S_{q2})i_q = \frac{3}{5} I_{dc} \\ \frac{3}{5} C \frac{dU_{C4}}{dt} - (S_{d7} + S_{d8})i_d - (S_{q7} + S_{q8})i_q = \frac{3}{5} I_{dc} \end{cases} \quad (4)$$

where  $i_d$  and  $i_q$  are the three-phase current in the rotation  $d$ - $q$  frame;  $U_{ed}$  and  $U_{eq}$  are the grid-connected voltage in the rotation  $d$ - $q$  frame;  $S_{d1}$ ,  $S_{q1}$  and  $S_{d2}$ ,  $S_{q2}$  are the coordinate components of  $S_{A1}$  and  $S_{A2}$  in the rotation  $d$ - $q$  frame;  $S_{d7}$ ,  $S_{q7}$  and  $S_{d8}$ ,  $S_{q8}$  are the coordinate components of  $S_{A7}$  and  $S_{A8}$  in the rotation  $d$ - $q$  frame; and  $\omega$  is the angular speed of rotation.

### 3. SPWM Modulation Strategy

Sinusoidal pulse width modulation (SPWM) strategies have been used widely for the switching of multilevel inverters due to their simplicity, flexibility, and reduced computational requirements compared to space vector modulation (SVM). Multilevel voltage source inverter systems offer the advantages of realizing higher voltages using smaller rating switching devices; they also achieve better quality output voltage waveforms compared to the use of two-level inversion systems. There are different modulation techniques based on the SPWM scheme; the carrier-based modulation schemes for multilevel inverters require carrier signals. They can be generally classified into two categories: phase-shifted and level-shifted modulations. In phase-shifted modulation, all the triangular carriers have the same frequency and the same amplitude, but there is a phase shift angle between any two adjacent carrier waves.

There are basically three types of schemes for the level-shifted modulation, which are as follows: In-phase disposition (IPD), Alternative phase opposite disposition (APOD), and Phase opposite disposition (POD). In the In-phase disposition (IPD) modulation, see Figure 2, each phase uses a sinusoidal modulation wave to compare a plurality of triangular carrier waves in a multilevel inverter. When the amplitude of the sine wave is greater than the amplitude of the carrier wave, the switch is closed. On the contrary, when the amplitude of the sine wave is lower than the amplitude of the carrier wave, the switch is opened.

In Figure 2,  $V_a$  is the amplitude of the sinusoidal modulation wave, and  $V_1$  to  $V_4$  are the amplitudes of the same phase triangular wave. Among them,  $V_1$  controls  $T_{A1}$  and  $T_{A5}$ ,  $V_2$  controls  $T_{A2}$  and  $T_{A6}$ ,  $V_3$  controls  $T_{A3}$  and  $T_{A7}$ , and  $V_4$  controls  $T_{A4}$  and  $T_{A8}$ . When the amplitude of the sine wave  $V_a$  is greater than the amplitude of the triangular carrier wave  $V_1$  to  $V_4$ , the switching of each phase is shut down. On the contrary, when  $V_a$  is smaller than  $V_1$  to  $V_4$ , the switching is switched on.

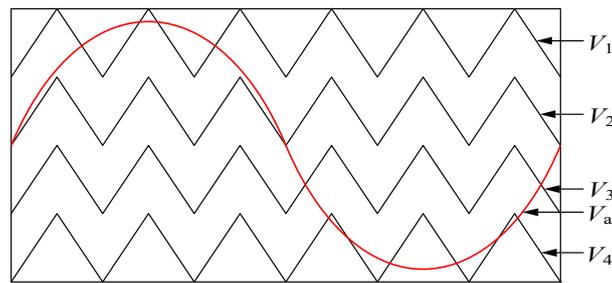


Figure 2. Comparison of modulation wave and carrier wave.

#### 4. Design of Passive Controller

##### 4.1. Passive E-L Model of the Five-Level Inverter

Selecting the system's state variables:

$$\mathbf{x} = \begin{bmatrix} x_1 & x_2 & x_3 & x_4 \end{bmatrix} = \begin{bmatrix} i_d & i_q & U_{C1} & U_{C4} \end{bmatrix} \quad (5)$$

Defining the energy storage function of the system:

$$H(\mathbf{x}) = (x_1^2 + x_2^2 + x_3^2 + x_4^2)/2 \quad (6)$$

Equation (4) is written in the form of the E-L equation under passivity-based controls (see Figure 1) [35,36].

$$M\dot{\mathbf{x}} + J\mathbf{x} + R\mathbf{x} = \mathbf{u} \quad (7)$$

Among them,

$$\mathbf{u} = \begin{bmatrix} -U_{ed} \\ -U_{eq} \\ \frac{3}{5}I_{dc} \\ \frac{3}{5}I_{dc} \end{bmatrix}, \mathbf{M} = \begin{bmatrix} L_f & 0 & 0 & 0 \\ 0 & L_f & 0 & 0 \\ 0 & 0 & \frac{3}{5}C & 0 \\ 0 & 0 & 0 & \frac{3}{5}C \end{bmatrix}, \mathbf{J} = \begin{bmatrix} 0 & -\omega L_f & -(S_{d1} + S_{d2}) & S_{d7} + S_{d8} \\ \omega L_f & 0 & -(S_{q1} + S_{q2}) & S_{q7} + S_{q8} \\ S_{d1} + S_{d2} & S_{q1} + S_{q2} & 0 & 0 \\ -(S_{d7} + S_{d8}) & -(S_{q7} + S_{q8}) & 0 & 0 \end{bmatrix}, \mathbf{R} = \begin{bmatrix} R & 0 & 0 & 0 \\ 0 & R & 0 & 0 \\ 0 & 0 & 0 & 0 \\ 0 & 0 & 0 & 0 \end{bmatrix}$$

where  $\mathbf{x}$  is the state variable,  $\mathbf{u}$  is the control variable that reflects the exchange between the system and the external energy,  $\mathbf{M}$  is a positive diagonal matrix consisting of energy storage elements,  $\mathbf{J}$  is the anti-symmetric matrix that reflects the internal interconnection structure of the system,  $\mathbf{J}$  is equal to  $-\mathbf{J}^T$ , and  $\mathbf{R}$  is the symmetric matrix that reflects the dissipation characteristics of the system.

##### 4.2. Design of Passive E-L Model Controller

For an  $m$  input and  $m$  output system:

$$\begin{cases} \mathbf{x} = f(\mathbf{x}, \mathbf{u}) \\ \mathbf{y} = h(\mathbf{x}) \end{cases} \quad \mathbf{x}(0) = \mathbf{x}_0 \in \mathbb{R}^n \quad (8)$$

where  $\mathbf{x}$ ,  $\mathbf{u}$ , and  $\mathbf{y}$  are the state variables, input variables, and output variables of the system, respectively; the spaces are  $\mathbf{x} \in \mathbb{R}^n$ ,  $\mathbf{u} \in \mathbb{R}^m$ , and  $\mathbf{y} \in \mathbb{R}^m$ , respectively; and  $f$  is the local Lipschitz about  $(\mathbf{x}, \mathbf{u})$ .

If there is a semi-definite and continuously differentiable storage function  $H(\mathbf{x})$  and a positive definite function  $Q(\mathbf{x})$  for  $\forall t > 0$ , the dissipation inequality is satisfied:

$$H[\mathbf{x}(t)] - H[\mathbf{x}(0)] \leq \int_0^t \mathbf{u}^T \mathbf{y} d\tau - \int_0^t Q(\mathbf{x}) d\tau \quad (9)$$

or

$$\dot{H}(x) \leq \mathbf{u}^T \mathbf{y} - Q(x) \quad (10)$$

The system is strictly passive if the input  $\mathbf{u}$ , the output  $\mathbf{y}$  and the energy supply rate  $\mathbf{u}^T \mathbf{y}$  are established.

For the inverter system represented by Equation (4), we can set to its storage function as  $H(x) = \mathbf{x}^T \mathbf{M} \mathbf{x} / 2$ . Then it can be deduced:

$$\begin{aligned} \dot{H} &= \mathbf{x}^T \mathbf{M} \dot{\mathbf{x}} = \mathbf{x}^T (\mathbf{u} - \mathbf{J} \mathbf{x} - \mathbf{R} \mathbf{x}) \\ &= \mathbf{u}^T \mathbf{x} - \mathbf{x}^T \mathbf{R} \mathbf{x} \end{aligned} \quad (11)$$

Assuming that  $\mathbf{y} = \mathbf{x}$ ,  $Q(x) = \mathbf{x}^T \mathbf{R} \mathbf{x}$ , it can be concluded that the system satisfies the strict passive inequality.

If  $\mathbf{x}_e = \mathbf{x} - \mathbf{x}^*$ , it can be deduced from Equation (7):

$$\mathbf{M} \dot{\mathbf{x}}_e + \mathbf{J} \mathbf{x}_e + \mathbf{R} \mathbf{x}_e = \mathbf{u} - \mathbf{M} \dot{\mathbf{x}}^* - \mathbf{J} \mathbf{x}^* - \mathbf{R} \mathbf{x}^* \quad (12)$$

where  $\mathbf{x}^*$  is the desired equilibrium point in the system. It can be expressed as:

$$\mathbf{x}^* = \begin{bmatrix} x_1^* & x_2^* & x_3^* & x_4^* \end{bmatrix}^T = \begin{bmatrix} i_{dref} & i_{qref} & U_{C1ref} & U_{C4ref} \end{bmatrix}^T \quad (13)$$

where  $i_{dref}$  and  $i_{qref}$  are the expected components in the  $d$  and  $q$  axis of the three-phase current  $i_A$ ,  $i_B$ , and  $i_C$ .  $U_{C1ref}$  and  $U_{C4ref}$  are the expected voltages of the capacitors  $C_1$  and  $C_4$  in the DC side, respectively.

Generally, the method of injected damping can be used to control  $\mathbf{x}_e$  quickly becoming zero. The injected damping dissipation term is:

$$\mathbf{R}_d \mathbf{x}_e = (\mathbf{R} + \mathbf{R}_a) \mathbf{x}_e \quad (14)$$

where  $\mathbf{R}_a$  is a semi-definite diagonal matrix that is similar to the form of matrix  $\mathbf{R}$  and  $\mathbf{R}_a = [R_{a1} \ R_{a2} \ R_{a3} \ R_{a4}]$ . Equation (12) can be rewritten as:

$$\mathbf{M} \dot{\mathbf{x}}_e + \mathbf{J} \mathbf{x}_e + \mathbf{R}_d \mathbf{x}_e = \mathbf{u} - (\mathbf{M} \dot{\mathbf{x}}^* + \mathbf{J} \mathbf{x}^* + \mathbf{R} \mathbf{x}^* - \mathbf{R}_a \mathbf{x}_e) \quad (15)$$

In order to ensure the strict passivity of the system, we can select the control law:

$$\mathbf{u} = \mathbf{M} \dot{\mathbf{x}}^* + \mathbf{J} \mathbf{x}^* + \mathbf{R} \mathbf{x}^* - \mathbf{R}_a \mathbf{x}_e \quad (16)$$

When  $\mathbf{M} \dot{\mathbf{x}} + \mathbf{R}_d \mathbf{x}_e = 0$ , the error energy function is:

$$\dot{H}_g = \mathbf{x}_e^T \mathbf{M} \dot{\mathbf{x}}_e = -\mathbf{x}_e^T (\mathbf{R}_d + \mathbf{J}) \mathbf{x}_e < 0 \quad (17)$$

Combining Equation (4) with Equation (7) to solve Equation (16), it can be deduced:

$$\begin{cases} -U_{ed} = L_f \frac{di_{dref}}{dt} - \omega L_f i_q + R i_{dref} - R_{a1} (i_d - i_{dref}) - U_{C1} (S_{d1} + S_{d2}) + U_{C4} (S_{d7} + S_{d8}) \\ -U_{eq} = L_f \frac{di_{qref}}{dt} + \omega L_f i_d + R i_{qref} - R_{a2} (i_q - i_{qref}) - U_{C1} (S_{q1} + S_{q2}) + U_{C4} (S_{q7} + S_{q8}) \\ \frac{3}{5} I_{dc} = \frac{3}{5} C \frac{dU_{C1ref}}{dt} + (S_{d1} + S_{d2}) i_d + (S_{q1} + S_{q2}) i_q - (U_{C1} - U_{C1ref}) R_{a3} \\ \frac{3}{5} I_{dc} = \frac{3}{5} C \frac{dU_{C4ref}}{dt} - (S_{d7} + S_{d8}) i_d - (S_{q7} + S_{q8}) i_q - (U_{C4} - U_{C4ref}) R_{a4} \end{cases} \quad (18)$$

With  $u_d$  and  $u_q$ , the input signal from the SPWM algorithm can be obtained from Equation (4):

$$\begin{cases} u_d = (S_{d1} + S_{d2})U_{C1} - (S_{d7} + S_{d8})U_{C4} \\ u_q = (S_{q1} + S_{q2})U_{C1} - (S_{q7} + S_{q8})U_{C4} \end{cases} \quad (19)$$

Combined with the Equations (18) and (19), it can be deduced:

$$\begin{cases} u_d = -\omega L_f i_q + (R + R_{a1})i_{dref} - R_{a1}i_d + U_{ed} \\ u_q = \omega L_f i_d - R_{a2}i_q + U_{eq} \end{cases} \quad (20)$$

In summary, the block diagram of the system under passivity-based control can be established. In Figure 3, the  $q$ -axis desired current  $i_{qref}$  is equal to 0 in order to ensure that the unit power factor is connected to the grid. The  $d$ -axis desired current  $i_{dref}$  is obtained by the difference between the actual capacitor voltage and the expected capacitor voltage through PI control.

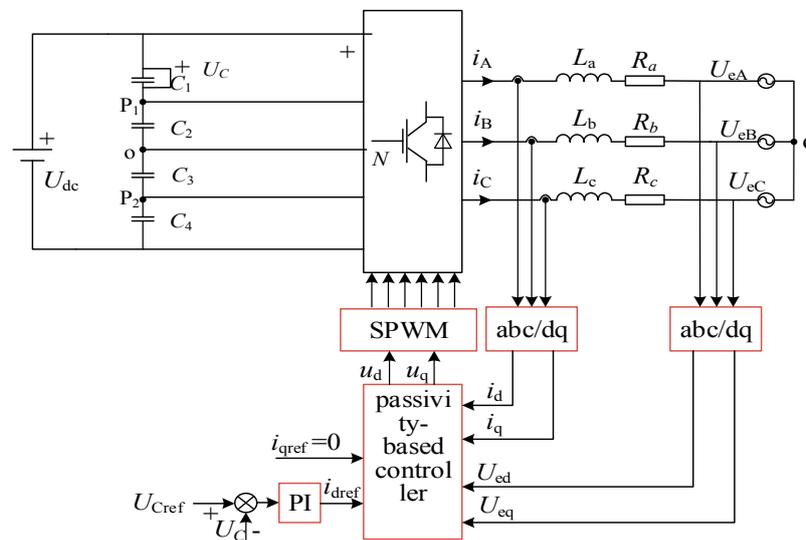


Figure 3. The block diagram of the system.

## 5. Software Simulation

### 5.1. Simulation of Passivity Control Mentioned in This Paper

According to the above analysis, a simulation model of passivity-based control based on the E-L model is built in Matlab/Simulink simulation software. The simulation parameter specifications are given in Table 1.

Table 1. Simulation parameters.

Parameter	Value	Parameter	Value
$U_{dc}$	600 V	$L_f$	1 mH
$C_1$ ( $C_2$ $C_3$ $C_4$ )	220 $\mu$ F	$R$	1 $\Omega$
$C$	50 $\mu$ F	$U_{eA}$ $U_{eB}$ $U_{eC}$	311 V
$L$	500 mH	frequency ( $f$ )	50 HZ

The output phase voltage and line voltage waveform of the inverter are presented in Figure 4a,b, respectively. It can be seen from Figure 4a that the phase voltage, which consists of +300 V, +150 V, 0 V, -150 V, and -300 V, is respectively close to the five levels of the inverter output in theory, which are

$+U_{dc}/2$ ,  $+U_{dc}/4$ ,  $0$ ,  $-U_{dc}/4$ , and  $-U_{dc}/2$ . Similarly, Figure 4b shows that the line voltage consists of  $+600$  V,  $+450$  V,  $+300$  V,  $+150$  V,  $0$  V,  $-150$  V,  $-300$  V,  $-450$  V, and  $-600$  V, which is respectively close to the nine levels of the inverter output in theory, which are  $+U_{dc}$ ,  $+U_{dc}3/4$ ,  $+U_{dc}/2$ ,  $+U_{dc}/4$ ,  $0$ ,  $-U_{dc}/4$ ,  $-U_{dc}/2$ ,  $-U_{dc}3/4$ , and  $-U_{dc}$ .

The outputs functions  $u_d$  and  $u_q$  from the passive controller, when the injection damping  $R_{a1} = R_{a2} = R_a = 5 \Omega$ ,  $15 \Omega$ ,  $25 \Omega$ ,  $50 \Omega$ , and  $100 \Omega$ , are shown in Figure 4c,d, respectively. In Figure 4c, when  $R_a \leq 25 \Omega$ ,  $u_d$  tends to be stable at about  $0.005$  s, and, when  $R_a > 25 \Omega$ , the stability time of  $u_d$  is significantly greater than  $0.01$  s. Among them, when  $R_a = 50 \Omega$ ,  $u_d$  tends to be stable at about  $0.02$  s, and, when  $R_a = 100 \Omega$ , the stability time is about  $0.04$  s.

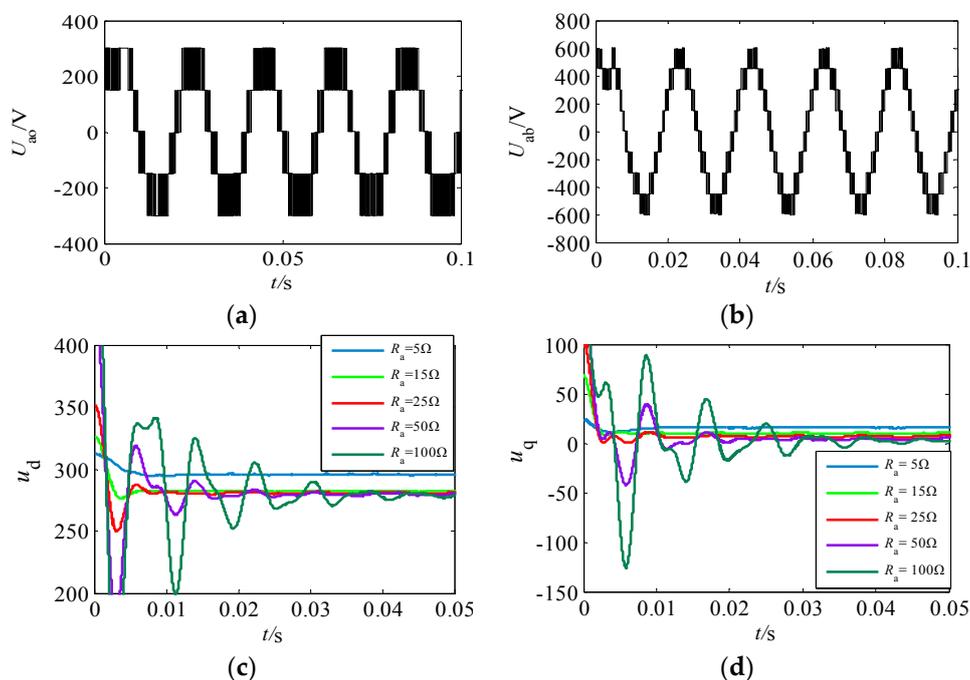
In Figure 4d, when  $R_a \leq 25 \Omega$ ,  $u_q$  tends to be stable about  $0.01$  s, and the stability time of the output function  $u_q$  is longer than  $0.01$  s, when  $R_a > 25 \Omega$ . Especially, when  $R_a = 50 \Omega$ ,  $u_q$  tends to be stable at about  $0.02$  s, and, when  $R_a = 100 \Omega$ ,  $u_q$  does not reach stability at  $0.04$  s.

Considering the steady-state response speed of the system, it is reasonable to select  $R_{a1} = R_{a2} = R_a = 25 \Omega$ .

Table 2 is the result of the steady-state time between  $U_d$  and  $U_q$ .

**Table 2.** Stability time of  $u_d$  and  $u_q$ .

Injection Damping	Stability Time of $u_d$	Stability Time of $u_q$
$R_a = 5 \Omega$	0.006 s	0.005 s
$R_a = 15 \Omega$	0.005 s	0.005 s
$R_a = 25 \Omega$	0.005 s	0.006 s
$R_a = 50 \Omega$	0.02 s	0.02 s
$R_a = 100 \Omega$	0.04 s	0.045 s



**Figure 4.** Simulation of passivity-based control. (a) Phase voltage of the inverter; (b) Line voltage of the inverter; (c) The output function  $u_d$ ; and (d) The output function  $u_q$ .

## 5.2. The Passivity-Based Control of This Paper Is Compared with the Traditional PI Control

In order to demonstrate the advantages of the passivity-based control proposed in this paper, this paper compares it with traditional PI control. Among these, the input of the PI controller of

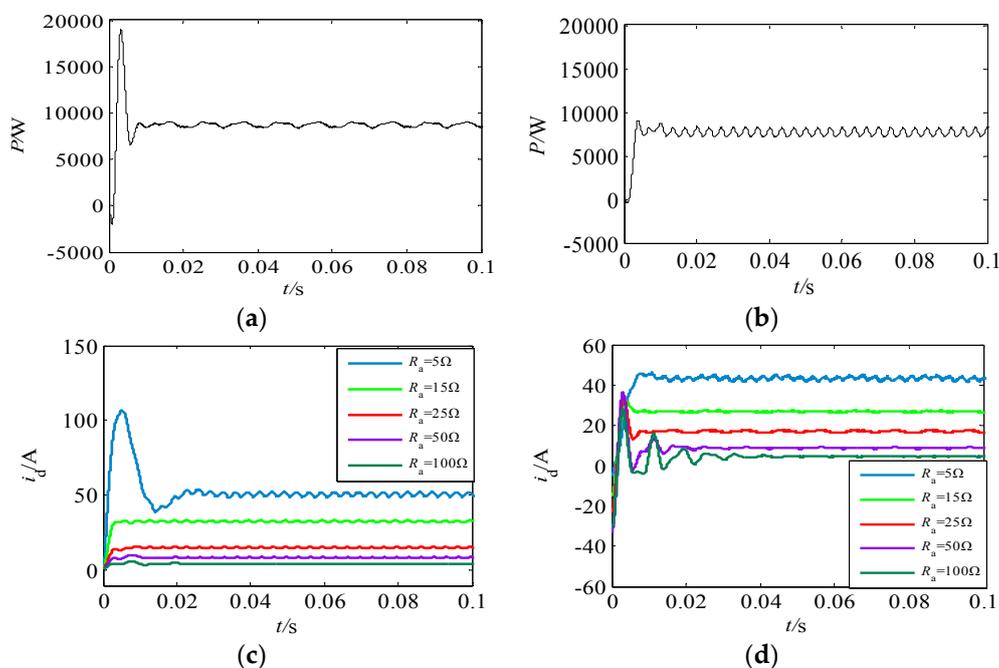
the voltage loop is the difference between the actual capacitor voltage and the reference capacitor voltage, and the main purpose is to track the capacitor voltage and inhibit the capacitor voltage offset. Meanwhile, the value of  $K_p$  is relatively small and the value of  $K_i$  is relatively large, which ensures the accuracy of voltage tracking. The function of the PI controller of the current loop is to track the three-phase grid current and voltage. If  $K_p$  is too large, the stability of the system is poor. In summary, we select  $K_p = 0.8$  and  $K_i = 5$ .

The active power  $P$  from the inverter is shown in Figure 5a,b under two strategies. As can be seen from the figure,  $P$  tends to be stable at about 0.01 s, and the stability value is close to 8000 W under the two control strategies. However, the amplitude fluctuations of the active power in Figure 5b are obviously larger than those in Figure 5a. It can be concluded that the static stability of the passivity-based control strategy is good.

The currents in the  $d$ -axis direction inside the passive controller under different injection dampings that are shown in Figure 5c are obtained by the three-phase current of the inverter through the abc-dq coordinate transformation. It can be observed in Figure 5c, with the increase of the injection damping, that the stability time of the current  $i_d$  is getting smaller and smaller. Especially, when  $R_a \geq 25 \Omega$ , the stability time is close to 0.003 s. Meanwhile, the fluctuation range of  $i_d$  is getting smaller, and the dynamic stability is getting higher.

The resistances in the traditional PI control system are set to 5  $\Omega$ , 15  $\Omega$ , 25  $\Omega$ , 50  $\Omega$ , and 100  $\Omega$ , which is contrast with the dynamic simulation of different injection dampings under the passivity-based control strategy. Figure 5d shows that the current  $i_d$  is under different resistances in the traditional PI control system. It can be seen from Figure 5d that, when  $R_a \leq 25 \Omega$ ,  $i_d$  tends to be stable at 0.01 s. When  $R_a = 50 \Omega$ ,  $i_d$  tends to be stable at about 0.02 s, and, when  $R_a = 100 \Omega$ ,  $i_d$  does not reach stability at 0.04 s.

Compared with Figure 5c, the stability time of the current  $i_d$  is significantly longer in Figure 5d. Meanwhile, the magnitude of the current amplitude fluctuates considerably in Figure 5c. In summary, the dynamic stability of passivity-based control is better than that of traditional PI control.

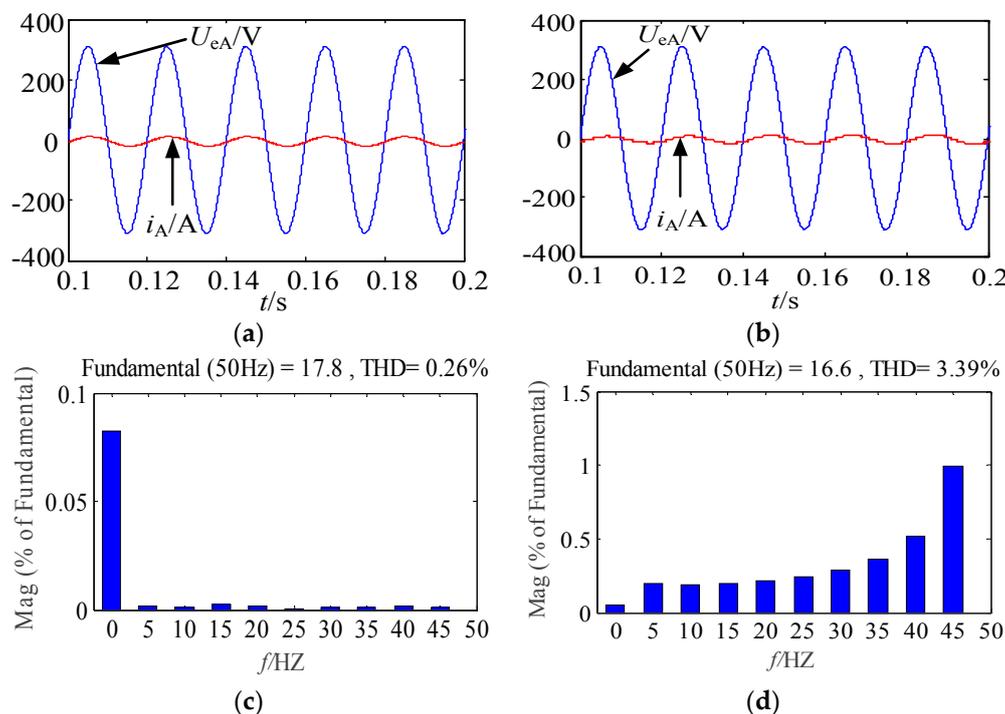


**Figure 5.** Comparison of static and dynamic stability under two strategies. (a) The output active power of the inverter under a passivity-based control (PBC) strategy; (b) The output active power of the inverter under the traditional PI control strategy; (c) The  $d$ -axis current under a PBC strategy; and (d) The  $d$ -axis current under the traditional PI control strategy.

A-phase grid voltage and current are shown in Figure 6a,b under two kinds of strategies. In Figure 6b, the current tends to be stable at about 0.1 s, and there is a certain phase difference between the grid voltage and current after stabilization. At this point, the system's power factor is very low. However, the grid current achieves stability in a very short period of time in Figure 6a. Meanwhile, there is a smaller phase difference between the grid voltage and current; thus the system's power factor is higher.

Figure 6c,d compares the harmonics of the grid currents controlled by the PBC strategy and the traditional PI control methods. It can be seen from the two figures that the harmonics of the A-phase current are 0.26% and 3.39% under two strategies, respectively. The results show that the typical harmonic in the grid current by the PBC method is smaller than that by the traditional PI control method due to the superior stability performance.

Table 3 shows the stability and harmonic results of the two control strategies.



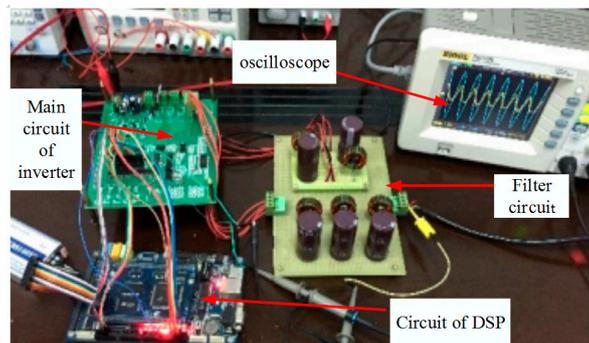
**Figure 6.** Comparison of phase and harmonics in two strategies; (a) A-phase grid voltage and current under a passivity-based control strategy; (b) A-phase grid voltage and current under the traditional PI control strategy; (c) A-phase current harmonics of the inverter under a passivity-based control strategy; and (d) A-phase current harmonics of the inverter under the traditional PI control strategy.

**Table 3.** Comparison of the two control strategies.

Parameter	PBC		Traditional PI	
	Stability Time	Amplitude of Fluctuation	Stability Time	Amplitude of Fluctuation
$p$	0.01 s	smaller	0.01 s	larger
$R_a = 5 \Omega$	0.02 s	smaller	0.01 s	larger
$R_a = 15 \Omega$	0.003 s	smaller	0.01 s	larger
$R_a = 25 \Omega$	0.003 s	smaller	0.01 s	larger
$R_a = 50 \Omega$	0.004 s	smaller	0.02 s	smaller
$R_a = 100 \Omega$	0.004 s	smaller	0.04 s	smaller
THD (%)		0.26		3.39

## 6. Prototype Experiment

In order to further illustrate the advantages of this method, this paper also builds the hardware experiment platform of the inverter. Meanwhile, an experimental analysis based on passivity-based control is also carried out on this platform. In the experiment, the micro-power supply is replaced by the DC power supply. The control signal is generated by the Digital Signal Processingn (DSP) controller of the TMS320F28335 (Texas Instruments, Dallas, TX, USA) type, and the switching device is the Infineon IKW40N120H3 (TrenchStop, Infineon, Germany). Meanwhile, the hard experiments using the same simulation specifications are given Table 1. The hardware experiment is shown in Figure 7.



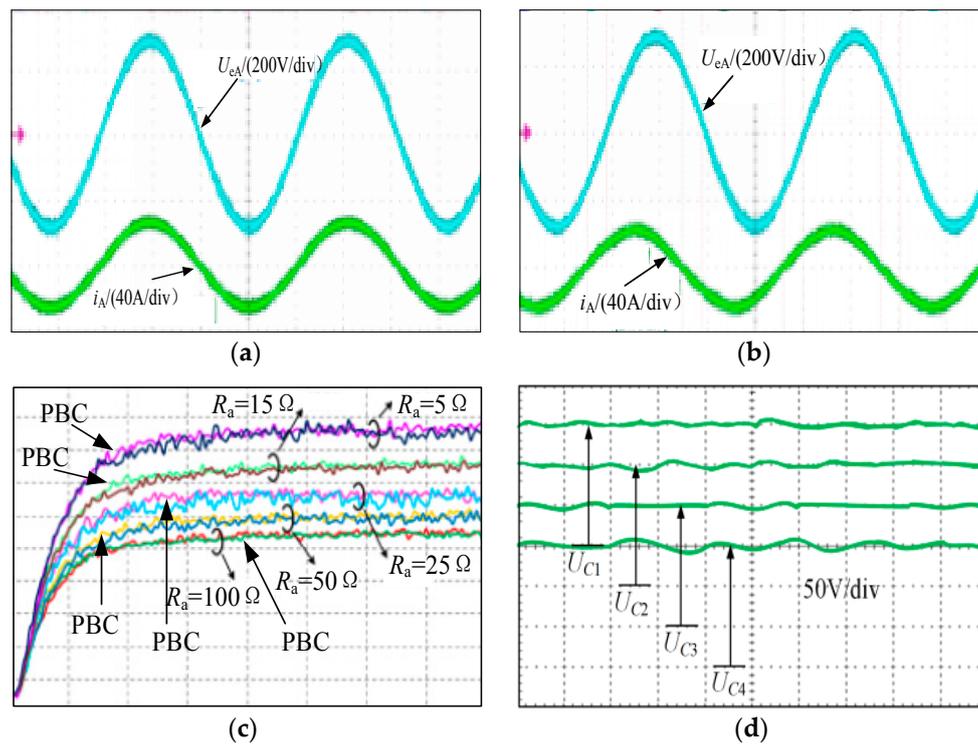
**Figure 7.** Photo of the hardware experimental platform.

The A-phase grid voltage and current are shown in Figure 8a,b under two kinds of strategies. In Figure 8a, the A-phase grid voltage is substantially in the same phase with the current of the inverter. At this point, the system has a better grid power factor. However, there is a certain phase difference between grid voltage and the current in Figure 8b. Therefore, the system's power factor is higher under the passivity-based control strategy. Meanwhile, compared with the software simulation, the voltage and current in Figure 8a are approximately consistent with the waveform in Figure 6a, which proves that the passive control strategy has a higher power factor. The waveform of voltage and current is affected proportional to the parameters and integral parameters in the PI controller, and it is difficult to find the most accurate PI parameters that meet the control requirements. Therefore, there is a phase difference between the voltage and the current of Figures 6b and 8b.

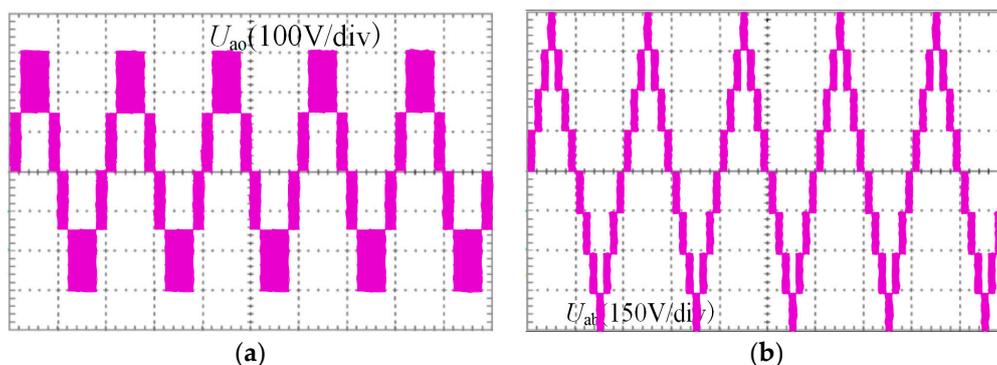
Figure 8c shows the  $d$ -axis current in the two kinds of strategies under different injection damping, which is obtained by the three-phase current of the inverter through the abc-dq coordinates transformation. In the Figure 8c, there is a certain fluctuation after the current reaches the stability under the two strategies. Especially, when  $R_a \leq 25 \Omega$ , the magnitude of the current amplitude fluctuates considerably. However, the ring of the fluctuation is significantly smaller under the PBC strategy, which proves that a passivity-based control strategy has good dynamic stability.

Figure 8d shows the polar film capacitor voltage under the PBC strategy. Here,  $U_{C1}$ ,  $U_{C2}$ ,  $U_{C3}$ , and  $U_{C4}$  are the voltages of the capacitors  $C_1$ ,  $C_2$ ,  $C_3$ , and  $C_4$  in the DC side, respectively. The capacitor voltage in the figure is close to 150 V, which proves that the problem of the balance of the neutral point is relatively small.

The output phase voltage and the line voltage waveform of the inverter are presented in Figure 9a,b, respectively. It can be seen from Figure 9a that the output phase voltage consisted of +300 V, +150 V, 0 V, -150 V, and -300 V and is close to the five levels of the inverter output in theory, which are  $+U_{dc}/2$ ,  $+U_{dc}/4$ , 0,  $-U_{dc}/4$ , and  $-U_{dc}/2$ . Similarly, Figure 9b shows that the output line voltage consists of +600 V, +450 V, +300 V, +150 V, 0 V, -150 V, -300 V, -450 V, and -600 V. Meanwhile, the experimental results are approximately consistent with the results obtained in the software simulation.



**Figure 8.** Comparison of hardware experiments under two strategies; (a) A-phase grid-connected voltage and current under a PBC strategy; (b) A-phase grid-connected voltage and current under the traditional PI control strategy; (c) The  $d$ -axis current of different injection dampings under the two control strategies; and (d) The polar film capacitor voltage under a PBC strategy.



**Figure 9.** Phase voltage and line voltage of the inverter; (a) Phase voltage of the inverter; and (b) Line voltage of the inverter.

## 7. Conclusions

This paper is related to a grid-connected control strategy of the five-level inverter based on a passive E-L model. Firstly, the mathematical model of the five-level inverter is deduced through the topological structure and the switching function. Then, the passive control law can be derived by selecting the appropriate energy function and the injection damping, which combines with the SPWM algorithm to drive the switch. Finally, the software simulation and hardware experiments draw the following conclusions:

- (1) The optimum stability of the system can be achieved by selecting the appropriate energy function and injection damping.

- (2) Compared with the traditional PI control method, the passivity-based control strategy has better static and dynamic stability and makes the system achieve a higher power factor.
- (3) In terms of economy, the harmonic loss very small under passivity-based control.

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